

UNITED STATES PATENT APPLICATION

**VOLTAGE CONTROLLED OSCILLATOR APPARATUS, METHOD, AND
SYSTEM**

INVENTOR

Waleed Khalil

LeMoine Patent Services, PLLC
c/o PortfolioIP
P.O. Box 52050
Minneapolis, MN 55402
ATTORNEY DOCKET 80107.097US1
Client Reference P17898

VOLTAGE CONTROLLED OSCILLATOR APPARATUS, METHOD, AND SYSTEM

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Field

The present invention relates generally to oscillator circuits, and more specifically to voltage controlled oscillator circuits.

Background

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Voltage controlled oscillators (VCOs) provide a VCO output signal having a frequency that varies based on a control signal. Voltage controlled oscillators may exhibit “phase noise,” which is a measure of how much the VCO output signal deviates from a pure sine wave at a single frequency.

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Brief Description of the Drawings

Figure 1 shows a diagram of a voltage controlled oscillator having isolated gate transistors;

Figure 2 shows a diagram of a voltage controlled oscillator having bipolar junction transistors;

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Figure 3 shows a diagram of a voltage controlled oscillator having isolated gate transistors and bipolar junction transistors;

Figure 4 shows a diagram of a circuit having gain devices with separate current sources;

Figure 5 shows a diagram of a frequency synthesizer;

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Figure 6 shows a system diagram in accordance with various embodiments of the present invention; and

Figure 7 shows a flowchart in accordance with various embodiments of the present invention.

Description of Embodiments

In the following detailed description, reference is made to the accompanying drawings that show, by way of illustration, specific embodiments in which the invention may be practiced. These embodiments are described in sufficient detail to enable those skilled in the art to practice the invention. It is to be understood that the various embodiments of the invention, although different, are not necessarily mutually exclusive. For example, a particular feature, structure, or characteristic described herein in connection with one embodiment may be implemented within other embodiments without departing from the spirit and scope of the invention. In addition, it is to be understood that the location or arrangement of individual elements within each disclosed embodiment may be modified without departing from the spirit and scope of the invention. The following detailed description is, therefore, not to be taken in a limiting sense, and the scope of the present invention is defined only by the appended claims, appropriately interpreted, along with the full range of equivalents to which the claims are entitled. In the drawings, like numerals refer to the same or similar functionality throughout the several views.

Figure 1 shows a diagram of a voltage controlled oscillator (VCO) having isolated gate transistors. Voltage controlled oscillator 100 includes inductor 110, varactors 120 and 130, isolated gate transistors 140 and 150, and current source 160. Inductor 110 and varactors 120 and 130 form an LC tank circuit. Isolated gate transistors 140 and 150 are shown as N-type metal oxide semiconductor field effect transistors (MOSFETs) having source nodes coupled in common, and each has a gate node coupled to the other's drain node. This configuration of transistors is referred to herein as a "cross-coupled" pair of transistors.

Voltage controlled oscillator 100 provides an oscillating signal (V_{OUT}) on nodes 104 and 106 that varies in frequency as the control voltage (V_{CTL}) on input node 102 changes. The frequency of V_{OUT} is set generally by the resonant frequency of the tank circuit, which is set by the inductance of inductor 110 and the capacitance of varactors 120 and 130, as well as other distributed reactive and resistive elements throughout VCO 100. As the control voltage V_{CTL} is varied on

input node 102, the capacitance of varactors 120 and 130 changes, the resonant frequency of the tank circuit changes, and the frequency of V_{OUT} changes.

Voltage controlled oscillator 100 also includes current source 160. Current source 160 sources a bias current I_{BIAS} that is provided to cross-coupled transistors 140 and 150. Values for I_{BIAS} and rationale for setting I_{BIAS} are described below.

Figure 2 shows a diagram of a voltage controlled oscillator having bipolar junction transistors (BJTs). Voltage controlled oscillator 200 includes the same LC tank circuit shown in Figure 1, but includes cross-coupled bipolar junction transistors 240 and 250 in place of isolated gate transistors 140 and 150. Voltage controlled oscillator 200 receives the control voltage (V_{CTL}) on node 102, and produces an output signal (V_{OUT}) on nodes 204 and 206. Voltage controlled oscillator 200 also includes current source 260 to source a bias current I_{BIAS} to the cross-coupled pair of bipolar junction transistors.

Voltage controlled oscillator 200 is referred to herein as a BJT VCO, in part because the cross-coupled transistors are BJT transistors. Further, VCO 100 (Figure 1) is referred to herein as a “MOSFET VCO” in part because the cross-coupled transistors in VCO 100 are shown as MOSFET devices.

As stated above, the MOSFET VCO and the BJT VCO each rely on a tuned LC tank circuit to control the frequency of oscillation. The tuned LC tank circuit suffers from finite loss due in part to resistive losses in the inductor and varactors. Each type of VCO also includes a cross-coupled gain stage (also referred to as a “ g_m stage”) to provide a “negative resistance” that overcomes the effect of the tank circuit loss. The gain stage is referred to as a g_m stage in part because the negative resistance is provided by the transconductance g_m of the cross-coupled transistors.

In general, the BJT has higher g_m for a given current and is well suited for high frequency applications. Accordingly, a large percentage of high performance VCOs are implemented as BJT VCOs. MOSFETs generally have a lower g_m and are better suited for lower frequency applications. Accordingly, MOSFET VCOs

are generally used in lower frequency applications or in places where designers have no access to BJT technology.

BIAS CURRENT CONSIDERATIONS

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Two different factors that may be considered to determine the bias level of a VCO circuit are the “startup condition” and the “amplitude condition.” These factors are described below along with their application to BJT and MOSFET VCOs.

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Startup Condition

One objective of the g_m stages is to simulate a negative resistance to the tank elements that compensate for the tank loss. In some embodiments, the minimum g_m of the transistor, ($g_{m\min}$), may be set to approximately three times
15 higher than the total loss (g_{loss}) of the tank elements:

$$g_{m\min} = 3g_{loss} \quad (\text{Eq. 1})$$

Where g_{loss} is equal to the reciprocal of the equivalent parallel resistance of
20 the tank circuit. The 3x factor may be used to ensure that under process and temperature variations, the VCO circuit will always have a higher g_m than the g_{loss} factor. Factors other than three may also be used. If the VCO circuit has a higher g_m than the g_{loss} , then the VCO will start to oscillate when power is applied. This is referred to herein as the condition for VCO startup.

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Amplitude Condition

Given a fixed tank loss, increasing the VCO output signal amplitude reduces the phase noise of the VCO. The VCO signal amplitude (V_{OUT}) is directly proportional to the bias current:

$$V_{OUT} = I_{BIAS} / g_{loss} \quad (\text{Eq. 2})$$

The manner in which g_m depends on bias current differs between BJTs and
 5 MOSFETs. For a BJT, g_m is directly proportional to the bias current:

$$g_{mBJT} = I_{BIAS} / V_t \quad (\text{Eq. 3})$$

where V_t is the thermal voltage. For a MOSFET, g_m has a weaker
 10 dependency on I_{BIAS} :

$$g_{mMOS} = \sqrt{K \cdot (W / L) \cdot I_{BIAS}} \quad (\text{Eq. 4})$$

where W = the width of the transistor and L = the length of the transistor.

15 In general, the square root factor applies to long channel devices where I_{BIAS} has a quadratic dependence on bias voltage. For short channel devices, this factor is even smaller translating to weaker current dependency. The transistor W/L sizing factor may be used to increase the g_m of the device, however, increasing W/L increases the loading capacitance and hence restricts the VCO operating frequency.

20 Because of differences in the transistor types, a factor of approximately ten times higher g_m can be achieved using a BJT circuit versus a reasonably sized MOSFET circuit. Since BJTs generally have a higher gain-bandwidth product (f_t) and a higher maximum frequency (f_{max}) than MOSFET transistors, their g_m frequency degradation factor is much lower. This leads to an important observation
 25 in terms of what sets the bias current upper bound for BJT VCOs versus MOSFET VCOs. In general BJT VCOs are bias limited by the VCO voltage swing condition (Eq. 2) and not the g_m startup condition (Eq. 1). Generally, BJT VCOs enjoy g_m

factors that are much higher than the required $g_{m\min}$. On the other hand, the g_m of MOSFET VCOs has weaker current dependency where both the bias current and W/L are optimized to obtain $g_{m\min}$ while not degrading the operating frequency of the VCO.

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NOISE CONSIDERATIONS

Voltage controlled oscillators may be used in many different applications, including in receive and transmit paths of radio circuits to down-convert or up-convert a modulated signal, respectively. This operation is often referred to as “mixing” where in an ideal case the VCO is modeled as a pure single tone signal. In practice, however, the VCO signal power has a noise skirt in the frequency domain. The power in this noise skirt is referred to as phase noise. Phase noise may be quantified in many ways, but is generally quoted in terms of dBc/Hz (phase noise in dB relative to the carrier amplitude per unit Hz) or Noise/Signal (N/S) per Hz.

Phase noise is generally undesirable. Decreasing phase noise may be achieved by 1) reducing the noise contribution of the VCO elements and/or 2) increasing the signal level. Option 2 is directly related to increasing the VCO bias current which results in higher power usage. Further, even if higher power usage is acceptable, the noise level of the VCO is positively correlated with the bias current, which reduces the effectiveness of increasing the current/signal level.

The thermal noise of the g_m transistors is a major limiting factor to the VCO phase noise. Thermal noise in a BJT is significantly different than in a MOSFET. For a BJT, thermal noise (shot noise) is directly proportional to current:

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$$I_{cNoise}^2 = 2q \cdot I_{BIAS} \quad (\text{Eq. 5})$$

For a MOSFET, thermal noise is directly proportional to g_m :

$$I_{dNoise}^2 = \gamma \cdot kT \cdot g_{mMOS} \quad (\text{Eq. 6})$$

where γ is a correction factor with values between about 0.5 and 2.

Comparing equations 5 and 6 (and using equation 4 to calculate g_{mMOS} versus I_{BIAS}), shows that thermal noise in a BJT is much higher than in a MOSFET at a given bias current.

Considering the fact that a high bias current for BJT was set to satisfy the voltage swing consideration (equation 2) and not the startup condition (equation 1), this leads to high BJT phase noise. Another observation to make is that the high bias current for the BJT VCO dictates a much higher g_m factor than what is required for the VCO startup. On the other hand, a MOSFET VCO utilizes the minimum g_m requirement for startup and enjoys a lower phase noise (equation 6).

As described above, BJT VCOs suffer from high phase noise due to the direct dependency of the thermal noise on bias current, and MOSFET VCOs have lower phase noise but suffer from low g_m and f_i / f_{max} . Low g_m and low f_i / f_{max} in MOSFETs translates to using higher bias currents or limiting their use in high frequency applications.

REDUCING PHASE NOISE

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Figure 3 shows a diagram of a voltage controlled oscillator having isolated gate transistors and bipolar junction transistors. Voltage controlled oscillator 300 includes the tank circuit shown in Figures 1 and 2, and also includes cross-coupled bipolar junction transistors 352 and 354, and cross-coupled isolated gate transistors 362 and 364. Cross-coupled isolated gate transistors 362 and 364 are shown as MOSFETs. The cross-coupled BJTs are coupled to current source 350 which provides a current $(\alpha \cdot I_{BIAS})$, and the cross-coupled MOSFETs are coupled to current source 360 which provides a current $(1 - \alpha)(I_{BIAS})$. The tank circuit has a

current of I_{BIAS} , which is equal to the sum of $(a \cdot I_{BIAS})$ and $(1 - a)(I_{BIAS})$. The “ a ” factor may be chosen to divide the bias current between the two cross-coupled transistor pairs.

Voltage controlled oscillator 300 utilizes the strengths of both BJT and MOSFET transistors. By combining the cross-coupled BJTs with cross-coupled isolated gate transistors, the phase noise of the resulting VCO is reduced. The bias current provided by current source 350 is set high enough for cross-coupled transistors 352 and 354 to satisfy the startup condition. This draws on the strength of the BJT (higher g_m), but keeps the bias current through the BJTs no larger than necessary, thereby reducing the phase noise contribution of the BJTs. Any desired output voltage swing is then achieved by providing additional current using current source 360. The phase noise contribution by the MOSFETs is kept small in part because the W/L factor may be kept small.

In some embodiments, the MOSFET stage is used to pass the majority of the bias current and reduce the BJT bias current and the BJT noise contribution. Since the BJT stage is able to provide the required $g_{m\min}$, in some embodiments the g_m of the additional MOSFET stage is kept low by using the minimum W/L required to pass the remaining bias current. Hence, low noise is also obtained from this additional MOSFET stage as a result of having low g_m (even with its high bias current). The small W/L for the MOSFET stage also reduces capacitive loading on the VCO tank circuit which reduces any shift in the oscillation frequency caused by capacitive loading.

When designing a VCO such as VCO 300, I_{BIAS} and “ a ” may be determined using the startup condition and amplitude condition described above. For example, I_{BIAS} may be set by the desired output voltage swing, also referred to as the “amplitude condition” (equation 2). Also for example, “ a ” may be selected such that the cross-coupled BJT transistors will pass the minimum required current to provide the startup $g_{m\min}$. In some embodiments, this current may be approximately 1/10th of the total bias current. This results in a lower thermal noise

contribution made by the cross-coupled BJTs (equation 5). In some embodiments, “ a ” may be increased beyond the point at which the minimum current required for startup is provided. For example, “ a ” may be increased to ensure that the startup condition is met over voltage and process variations.

5 The cross-coupled MOSFET transistors will pass the remaining bias current $(1 - a)I_{BIAS}$. The W/L sizing of the MOSFET transistors may be set to a much lower value since the MOSFETs are used to switch the remaining bias current to the tank, and not to provide the g_m for the VCO. This may also translate to a much lower thermal noise for the MOSFET devices (equation 6).

10 The isolated gate transistors shown in Figure 3 are shown as N-type metal oxide semiconductor field effect transistors (NMOSFETs), and the bipolar junction transistors are shown as NPN transistors. In some embodiments, P-type MOSFETs and PNP BJTs are utilized. In still further embodiments, other types of switching or amplifying elements may be utilized for the various transistors described herein,
15 without departing from the scope of the present invention.

 The circuits described herein may be manufactured in many different ways. For example, in some embodiments, VCO 300 is manufactured in a silicon germanium (SiGe) process.

 Figure 4 shows a diagram of a circuit having gain devices with separate
20 current sources. In some embodiments, circuit 400 represents a generalization of VCO 300 (Figure 3). Circuit 400 includes load circuit 410, first gain device 420, current source 422, second gain device 430, and current source 432. Load circuit 410 has a bias current I_{BIAS} passing through it, which is divided between first and second gain devices, 420 and 430, respectively. Current source 422 provides a bias
25 current $(a \cdot I_{BIAS})$, and current source 432 provides a bias current $(1 - a)I_{BIAS}$.

 Load circuit 410 may be any type of circuit that provides a load to the gain devices. Examples include, but are not limited to, active loads, tank circuits, or the like. In some embodiments, load circuit 410 includes a tank circuit that includes inductors and variable capacitors. One example embodiment of load circuit 410 is
30 shown in Figure 3 having inductor 110 and varactors 120 and 130.

First gain device 420 and second gain device 430 may have different characteristics. By utilizing separate gain stages with different characteristics, phase noise may be reduced. For example, first gain device 420 may have a higher transconductance than second gain device 430. Also for example, first gain device 420 may have exhibit a phase noise characteristic that shows a greater dependency on bias current than second gain device 430. By splitting the bias current between first gain device 420 and second gain device 430, a desired amount of gain may be achieved using a desired amount of bias current, while reducing phase noise.

In some embodiments, first gain device 420 includes cross-coupled bipolar junction transistors, and in some embodiments, second gain device 420 includes cross-coupled isolated gate transistors. Many different embodiments may exist having different combinations of gain element types.

In some embodiments, circuit 400 implements a voltage controlled oscillator. In other embodiments, circuit 400 represents an oscillator having a substantially fixed output frequency. In general, circuit 400 may be any circuit with multiple gain devices that have different characteristics.

Figure 5 shows a diagram of a frequency synthesizer. Frequency synthesizer 500 includes VCO 520, frequency prescaler 530, low pass filter (LPF) 512, and compare circuit 510. In operation, compare circuit 510 receives a reference signal on node 502, and an output signal from frequency prescaler 530. Compare circuit 510 may compare phases of the two signals or frequency of the two signals and produce an error signal. The error signal is received by LPF 512 which produces a VCO control signal. VCO 520 receives the VCO control signal from LPF 512, and produces an output signal on node 504.

Voltage controlled oscillator 520 may produce an output signal that is greater in frequency than the reference signal on node 502 in part because prescaler 530 divides the frequency of the output signal on node 504. Voltage controlled oscillator 520 may be any of the VCO embodiments described herein, including one of the embodiments represented by VCO 300 (Figure 3) or circuit 400 (Figure 4).

Prescaler 530 may be any type of suitable prescaler, including a prescaler capable of

dividing the frequency of the VCO output signal by a variable amount.

Figure 6 shows a system diagram in accordance with various embodiments of the present invention. System 600 includes frequency synthesizer 620, direct conversion receiver 610, and antenna 630. Frequency synthesizer 620 may include
5 any of the VCO embodiments described above. Further, frequency synthesizer 620 may be implemented using a circuit topology similar to that shown in Figure 5.

Frequency synthesizer 620 may provide a local oscillator signal on node 622, and direct conversion receiver 610 may receive a local oscillator signal at oscillator input port 612. Direct conversion receiver 610 may also receive a signal
10 from antenna 630. Direct conversion receiver 610 may utilize the local oscillator signal to “down-convert” the signal received from antenna 630 directly to baseband. Because direct conversion receiver 610 does not utilize an intermediate frequency (IF), it may also be referred to as a “zero-IF” receiver.

In some embodiments, system 600 includes a transceiver that both transmits
15 and receives signals at antenna 630. For example, system 600 may be a cell phone with a transmitter and a receiver. Also for example, system 600 may be a wireless local area network interface that includes both a transmitter and a receiver. In some embodiments, antenna 630 may be a directional antenna, and in other embodiments, antenna 630 may be an omni-directional antenna.

20 Frequency synthesizers (and VCOs) may be used in systems other than systems represented by Figure 6. For example, a frequency synthesizer may be used in a system that includes a heterodyne receiver that utilizes an intermediate frequency. Many other system uses exist for frequency synthesizers and VCOs.

Voltage controlled oscillators, frequency synthesizers, cross-coupled
25 transistors, and other embodiments of the present invention can be implemented in many ways. In some embodiments, they are implemented in integrated circuits as part of electronic systems. In some embodiments, design descriptions of the various embodiments of the present invention are included in libraries that enable designers to include them in custom or semi-custom designs. For example, any of the
30 disclosed embodiments can be implemented in a synthesizable hardware design

language, such as VHDL or Verilog, and distributed to designers for inclusion in standard cell designs, gate arrays, or the like. Likewise, any embodiment of the present invention can also be represented as a hard macro targeted to a specific manufacturing process. For example, portions of VCO 300 (Figure 3) may be
5 represented as polygons assigned to layers of an integrated circuit.

Figure 7 shows a flowchart in accordance with various embodiments of the present invention. In some embodiments, method 700, or portions thereof, is performed by a voltage controlled oscillator, embodiments of which are shown in previous figures. In other embodiments, method 700 is performed by a frequency
10 synthesizer, an integrated circuit, or an electronic system. Method 700 is not limited by the particular type of apparatus performing the method. The various actions in method 700 may be performed in the order presented, or may be performed in a different order. Further, in some embodiments, some actions listed in Figure 7 are omitted from method 700.

15 Method 700 is shown beginning with block 710 in which a first current is provided to a pair of cross-coupled bipolar junction transistors. In some embodiments, this corresponds to the operation of current source 350 (Figure 3). The magnitude of the first current may be large or small, and may be adequate to satisfy a VCO startup condition. Further, the magnitude of the first current may be
20 inadequate to satisfy an amplitude condition. For example, in some embodiments, the first current is just large enough to allow the transconductance of the bipolar junction transistors to overcome the loss of a tank circuit. For example, referring now back to Figure 3, current source 350 sources a current of $(a \cdot I_{BIAS})$, where I_{BIAS} is the total bias current through the tank circuit, and the “a” multiplier
25 represents the fraction of the total bias current that passes through the cross-coupled bipolar junction transistors. In embodiments represented by Figure 3, this fraction of the total bias current is equal to the first current referred to in 710.

At 720, a second current is provided to a pair of cross-coupled MOSFET transistors. In some embodiments, this corresponds to the operation of current
30 source 360 (Figure 3). The magnitude of the second current may be large or small,

but in some embodiments, the magnitude of the second current is set to provide a desired output amplitude swing on nodes 304 and 306 (Figure 3). In some embodiments, the “ α ” multiplier in Figure 3 is set to about 1/10. In these embodiments, 1/10 of the total bias current is provided to the pair of cross-coupled
5 bipolar junction transistors, and 9/10 of the total bias current is provided to the pair of cross-coupled MOSFET transistors.

At 730, the first and second currents are summed to form a third current, and at 740, the third current is provided to a tank circuit. This corresponds to the currents through the cross-coupled bipolar junction transistors and the cross-coupled
10 MOSFET transistors summing to form the total bias current which passes through the tank circuit as shown in Figure 3.

Although the present invention has been described in conjunction with certain embodiments, it is to be understood that modifications and variations may be resorted to without departing from the spirit and scope of the invention as those
15 skilled in the art readily understand. Such modifications and variations are considered to be within the scope of the invention and the appended claims.